

采用 2x2 DRV 封装的 TPS6229x 1A 降压转换器

1 特性

- 高效率 - 高达 96%
- 高达 1000mA 的输出电流
- V_{IN} 范围为 2.3V 至 6.0V，支持具有扩展电压范围的锂离子电池
- 2.25MHz 固定频率运行
- 轻载电流下的省电模式
- PWM 模式下的输出电压精度为 $\pm 1.5\%$
- 固定输出电压选项
- 静态电流典型值为 15 μ A
- 可实现最低压降的 100% 占空比
- 轻载时的电压定位
- 采用 2mm $\times$ 2mm $\times$ 0.8mm WSON (6) 封装 (DRV)

2 应用

- 移动电话、智能手机
- 无线 LAN
- 掌上电脑
- 低功耗 DSP 电源
- 便携式媒体播放器
- 负载点 (POL) 应用

3 说明

TPS6229x 器件是高效的同步降压直流/直流转换器，经优化可适用于电池供电的便携式应用。这些器件采用单块锂离子电池提供高达 1000mA 的输出电流。

凭借 2.3V 至 6.0V 的输入电压范围，这些器件支持具有扩展电压范围的电池，非常适合为便携式应用（如手机和其他便携式设备）供电。

TPS6229x 器件在 2.25MHz 的固定开关频率下运行，在轻载电流情况下会进入省电模式，以便在整个负载电流范围内保持高效率。

省电模式经过优化，具有低输出电压纹波。对于低噪声应用，可通过将 MODE 引脚的电平拉高来强制这些器件进入固定频率脉宽调制 (PWM) 模式。在关断模式下，流耗减少至 1 μ A 以下。TPS6229x 器件允许使用小型电感器和电容器，可实现较小的解决方案尺寸。

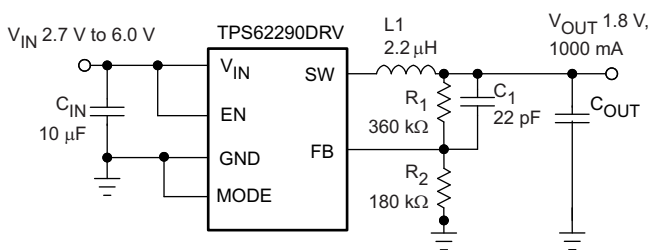
TPS6229x 器件在自然通风环境下的额定工作温度范围为 -40°C 至 85°C 。这些器件采用 2mm $\times$ 2mm 6 引脚 WSON 封装 (DRV)。

器件信息⁽¹⁾

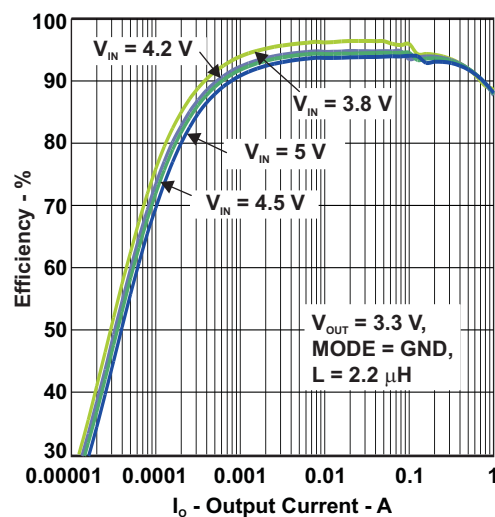
器件型号	封装	封装尺寸 (标称值)
TPS6229x	SON (6)	2.00mm $\times$ 2.00mm

(1) 如需了解所有可用封装，请参阅数据表末尾的可订购产品附录。

典型应用电路原理图



效率与输出电流间的关系



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4 修订历史记录

注：之前版本的页码可能与当前版本有所不同。

Changes from Revision F (January 2016) to Revision G	Page
• Changed Equation 3 operator from × to + in correcting the I_{Lmax} formula.	12
• Added cross references to the Third-party Products disclaimer.	12
Changes from Revision E (September 2015) to Revision F	Page
• Added Device Comparison Table	3
Changes from Revision D (November 2009) to Revision E	Page
• 已添加 引脚配置和功能 部分、ESD 额定值 表、特性 说明 部分、器件功能模式、应用和实施 部分、电源建议 部分、布局 部分、器件和文档支持 部分以及机械、封装和可订购信息 部分	1

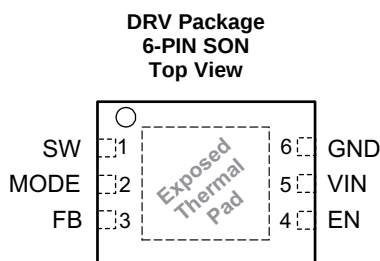
5 Device Comparison Table

PART NUMBER	OUTPUT VOLTAGE ⁽¹⁾	DEVICE MARKING ⁽²⁾
TPS62290	Adjustable	BYN
TPS62291	3.3 V fixed	CFY
TPS62293	1.8 V fixed	CFD

(1) Contact TI for other fixed output voltage options

(2) For the most current package and ordering information, see [机械、封装和可订购信息](#), or see the TI website at www.ti.com

6 Pin Configuration and Functions



Pin Functions

PIN		TYPE	DESCRIPTION
NAME	NO.		
EN	4	IN	This is the enable pin of the device. Pulling this pin to low forces the device into shutdown mode. Pulling this pin to high enables the device. This pin must be terminated.
FB	3	IN	Feedback pin for the internal regulation loop. Connect the external resistor divider to this pin. In case of fixed output voltage option, connect this pin directly to the output capacitor
GND	6	PWR	GND supply pin
MODE	2	IN	MODE pin = High forces the device to operate in fixed-frequency PWM mode. Mode pin = Low enables the power save mode with automatic transition from PFM mode to fixed-frequency PWM mode.
SW	1	OUT	This is the switch pin and is connected to the internal MOSFET switches. Connect the external inductor between this terminal and the output capacitor.
VIN	5	PWR	V _{IN} power supply pin.
Exposed Thermal Pad			Connect the exposed thermal pad to GND.

7 Specifications

7.1 Absolute Maximum Ratings

Over operating free-air temperature range (unless otherwise noted)⁽¹⁾

	MIN	MAX	UNIT
V _{IN} Input voltage range ⁽²⁾	−0.3	7	V
Voltage range at EN, MODE	−0.3	V _{IN} +0.3, ≤ 7	
Voltage at SW	−0.3	7	
Peak output current	Internally limited		A
T _J Maximum operating junction temperature	−40	125	°C
T _{stg} Storage temperature	−65	150	

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) All voltage values are with respect to network ground terminal.

7.2 ESD Ratings

	VALUE	UNIT
V _(ESD) Electrostatic discharge	Human body model (HBM), per ANSI/ESDA/JEDEC JS-001 ⁽¹⁾	±2000
	Charged-device model (CDM), per JEDEC specification JESD22-C101 ⁽²⁾	±1000

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
- (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

7.3 Recommended Operating Conditions

	MIN	NOM	MAX	UNIT
V _{IN} Supply voltage	2.3		6	V
Output voltage range for adjustable voltage	0.6		V _{IN}	V
T _A Operating ambient temperature	−40		85	°C
T _J Operating junction temperature	−40		125	°C

7.4 Thermal Information

THERMAL METRIC ⁽¹⁾		TPS6229x	UNIT
		DRV (SON)	
		6 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	67.8	°C/W
R _{θJC(top)}	Junction-to-case (top) thermal resistance	88.6	°C/W
R _{θJB}	Junction-to-board thermal resistance	37.2	°C/W
ψ _{JT}	Junction-to-top characterization parameter	2	°C/W
ψ _{JB}	Junction-to-board characterization parameter	37.6	°C/W
R _{θJC(bot)}	Junction-to-case (bottom) thermal resistance	7.9	°C/W

- (1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, [SPRA953](#).

7.5 Electrical Characteristics

Over full operating ambient temperature range, typical values are at $T_A = 25^\circ\text{C}$. Unless otherwise noted, specifications apply for condition $V_{IN} = EN = 3.6\text{ V}$. External components $C_{IN} = 4.7\text{ }\mu\text{F}$ 0603, $C_{OUT} = 10\text{ }\mu\text{F}$ 0603, $L = 2.2\text{ }\mu\text{H}$, refer to parameter measurement information.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
SUPPLY						
V _{IN}	Input voltage		2.3		6	V
I _{OUT}	Output current	V _{IN} 2.7 V to 6 V			1000	mA
		V _{IN} 2.5 V to 2.7 V			600	
		V _{IN} 2.3 V to 2.5 V			300	
I _Q	Operating quiescent current	I _{OUT} = 0 mA, PFM mode enabled (MODE = GND) device not switching, See ⁽¹⁾		15		μA
		I _{OUT} = 0 mA, switching with no load (MODE = V _{IN}) PWM operation, V _{OUT} = 1.8 V, V _{IN} = 3 V		3.8		mA
I _{SD}	Shutdown current	EN = GND		0.1	1	μA
UVLO	Undervoltage lockout threshold	Falling		1.85		V
		Rising		1.95		
ENABLE, MODE						
V _{IH}	High level input voltage, EN, MODE	2.3 V ≤ V _{IN} ≤ 6 V	1		V _{IN}	V
V _{IL}	Low level input voltage, EN, MODE	2.3 V ≤ V _{IN} ≤ 6 V	0		0.4	V
I _{IN}	Input bias current, EN, MODE	EN, MODE = GND or V _{IN}		0.01	1	μA
POWER SWITCH						
R _{DS(on)}	High side MOSFET on-resistance	V _{IN} = V _{GS} = 3.6 V, T _A = 25°C		240	480	mΩ
	Low side MOSFET on-resistance			185	380	
I _{LIMF}	Forward current limit MOSFET high-side and low side	V _{IN} = V _{GS} = 3.6 V	1.19	1.4	1.68	A
T _{SD}	Thermal shutdown	Increasing junction temperature		140		°C
	Thermal shutdown hysteresis	Decreasing junction temperature		20		
OSCILLATOR						
f _{SW}	Oscillator frequency	2.3 V ≤ V _{IN} ≤ 6 V	2.0	2.25	2.5	MHz
OUTPUT						
V _{OUT}	Adjustable output voltage range		0.6		V _I	V
V _{ref}	Reference voltage			600		mV
V _{FB(PWM)}	Feedback voltage PWM mode	MODE = V _{IN} , PWM operation, 2.3 V ≤ V _{IN} ≤ 6 V, See ⁽²⁾	−1.5%	0%	1.5%	
V _{FB(PFM)}	Feedback voltage PFM mode	MODE = GND, device in PFM mode, +1% voltage positioning active, See ⁽¹⁾		1%		
	Load regulation			−0.5		%/A
t _{start Up}	Start-up time	Time from active EN to reach 95% of V _{OUT}		500		μs
t _{Ramp}	V _{OUT} ramp-up time	Time to ramp from 5% to 95% of V _{OUT}		250		μs
I _{lkg}	Leakage current into SW pin	V _{IN} = 3.6 V, V _{IN} = V _{OUT} = V _{SW} , EN = GND, See ⁽³⁾		0.1	1	μA

(1) In PFM mode, the internal reference voltage is set to typical $1.01 \times V_{ref}$. See the parameter measurement information.

(2) For $V_{IN} = V_{OUT} + 1.0\text{ V}$

(3) In fixed output voltage versions, the internal resistor divider network is disconnected from FB pin.

7.6 Typical Characteristics

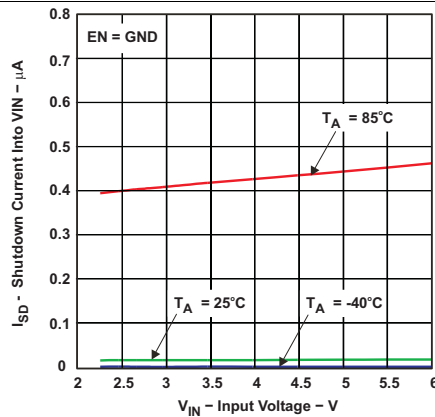


Figure 1. Shutdown Current Into VIN vs Input Voltage

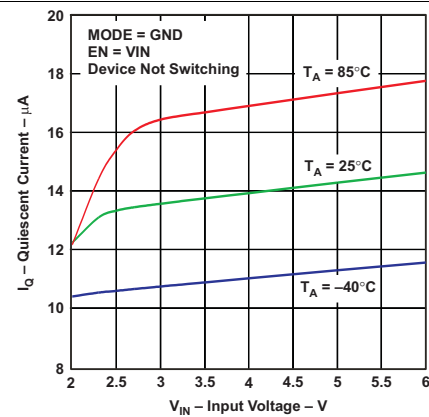


Figure 2. Quiescent Current vs Input Voltage

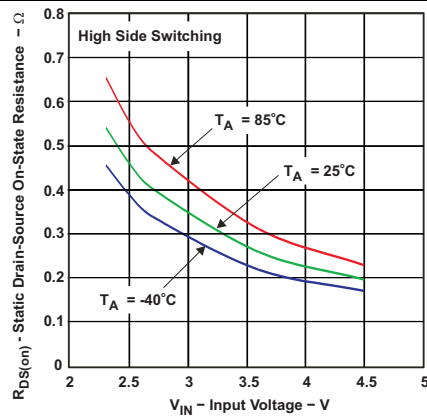


Figure 3. Static Drain-Source On-State Resistance vs Input Voltage

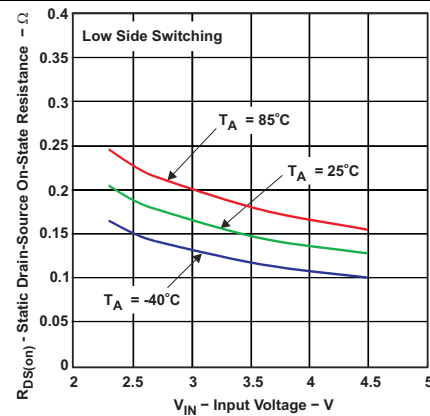


Figure 4. Static Drain-Source On-State Resistance vs Input Voltage

8 Detailed Description

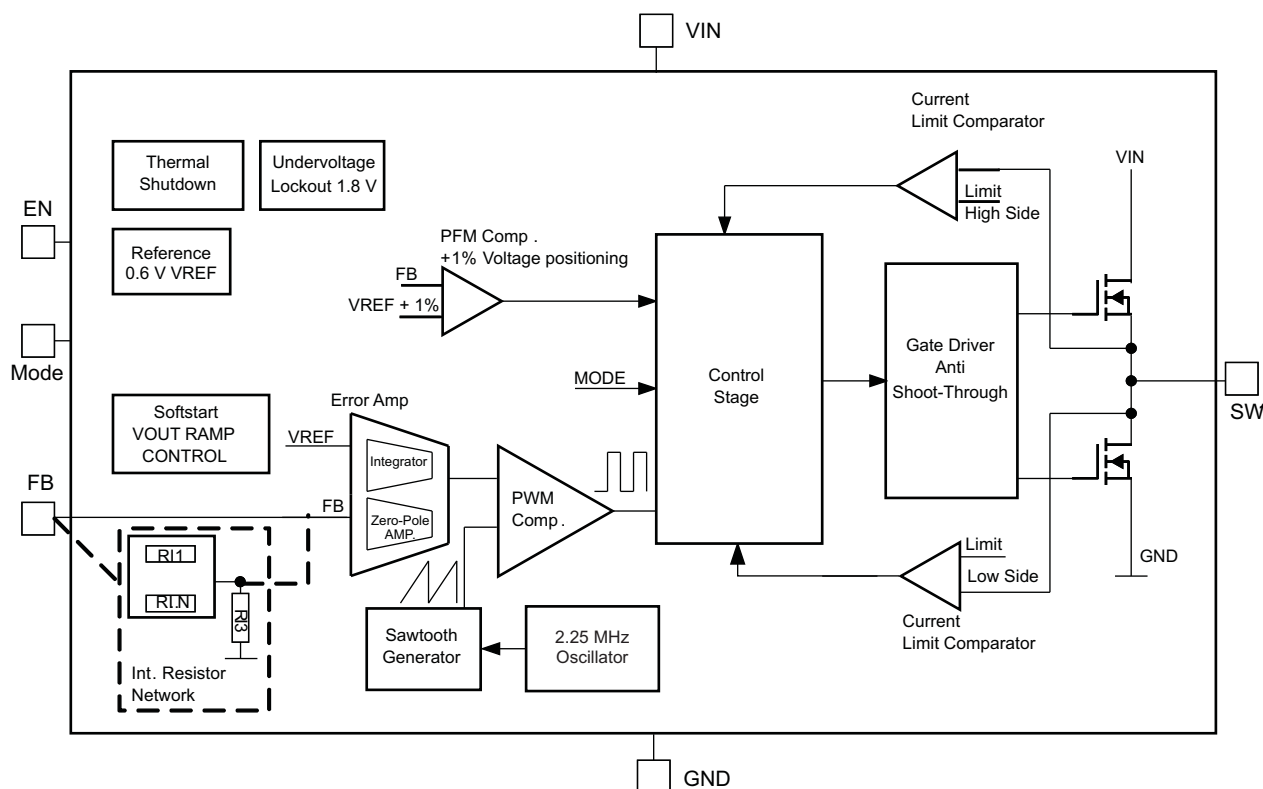
8.1 Overview

The TPS6229x step down converters operate with typically 2.25-MHz fixed frequency pulse width modulation (PWM) mode at moderate to heavy load currents. At light load currents, the converters can automatically enter power save mode and operate then in pulse frequency modulation (PFM) mode.

During PWM operation, the converters use a unique fast response voltage mode controller scheme with input voltage feed-forward to achieve good line and load regulation allowing the use of small ceramic input and output capacitors. At the beginning of each clock cycle initiated by the clock signal, the high side MOSFET switch is turned on. The current flows now from the input capacitor via the high side MOSFET switch through the inductor to the output capacitor and load. During this phase, the current ramps up until the PWM comparator trips and the control logic will turn off the switch. The current limit comparator also turns off the switch in case the current limit of the high side MOSFET switch is exceeded. After a dead time preventing shoot through current, the low side MOSFET rectifier is turned on and the inductor current ramps down. The current flows now from the inductor to the output capacitor and to the load. It returns to the inductor through the low side MOSFET rectifier.

The next cycle is initiated by the clock signal again turning off the low side MOSFET rectifier and turning on the high side MOSFET switch.

8.2 Functional Block Diagram



8.3 Feature Description

8.3.1 Dynamic Voltage Positioning

This feature reduces the voltage undershoots/overshoots at load steps from light to heavy load and vice versa. It is active in power save mode and regulates the output voltage 1% higher than the nominal value. This provides more headroom for both the voltage drop at a load step, and the voltage increase at a load throw-off.

Feature Description (continued)

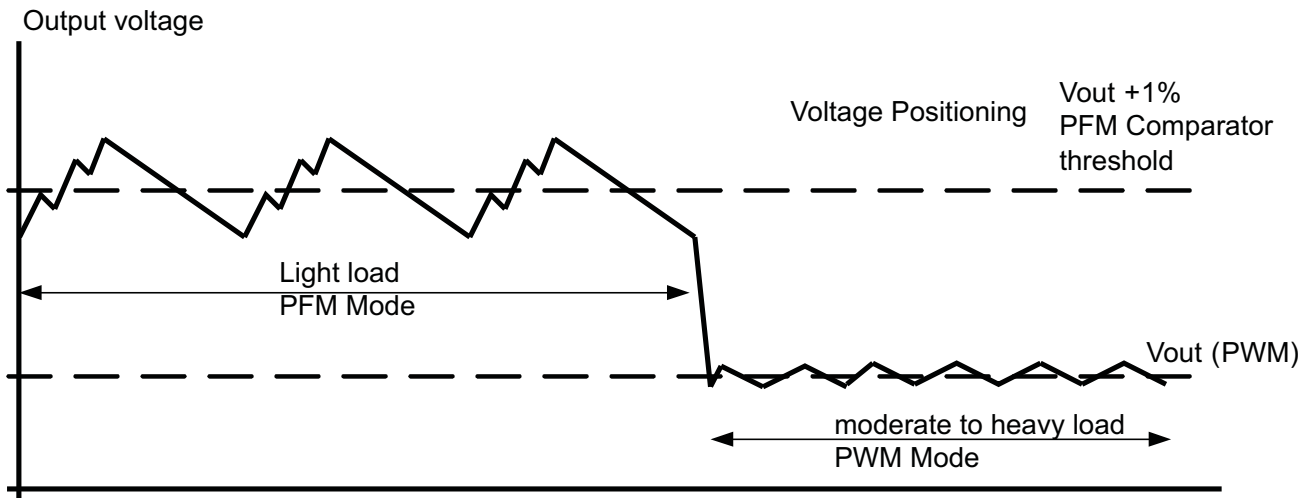


Figure 5. Power Save Mode Operation

8.3.2 Enable

The device is enabled by setting EN pin to high. During the start up time $t_{\text{Start Up}}$ the internal circuits are settled and the soft start circuit is activated. The EN input can be used to control power sequencing in a system with various DC/DC converters. The EN pin can be connected to the output of another converter, to drive the EN pin high and getting a sequencing of supply rails. With EN = GND, the device enters shutdown mode, in which all internal circuits are disabled. In fixed output voltage versions, the internal resistor divider network is disconnected from FB pin.

8.3.3 Mode Selection

The MODE pin allows mode selection between forced PWM mode and power save mode.

Connecting this pin to GND enables the power save mode with automatic transition between PWM and PFM mode. Pulling the MODE pin high forces the converter to operate in fixed frequency PWM mode even at light load currents. This allows simple filtering of the switching frequency for noise sensitive applications. In this mode, the efficiency is lower compared to the power save mode during light loads.

The condition of the MODE pin can be changed during operation and allows efficient power management by adjusting the operation mode of the converter to the specific system requirements.

8.3.4 Undervoltage Lockout

The undervoltage lockout circuit prevents the device from malfunctioning at low input voltages and from excessive discharge of the battery and disables the output stage of the converter. The undervoltage lockout threshold is typically 1.85 V with falling V_{IN} .

8.3.5 Thermal Shutdown

As soon as the junction temperature, T_J , exceeds 140°C (typical) the device goes into thermal shutdown. In this mode, the high side and low side MOSFETs are turned-off. The device continues its operation when the junction temperature falls below the thermal shutdown hysteresis.

8.4 Device Functional Modes

8.4.1 Soft-Start

The TPS6229x has an internal soft start circuit that controls the ramp up of the output voltage. The output voltage ramps up from 5% to 95% of its nominal value within typical 250 μ s. This limits the inrush current in the converter during ramp up and prevents possible input voltage drops when a battery or high impedance power source is used. The soft start circuit is enabled within the start up time $t_{Start Up}$.

8.4.2 Power Save Mode

The power save mode is enabled with MODE pin set to low level. If the load current decreases, the converter will enter power save mode operation automatically. During power save mode the converter skips switching and operates with reduced frequency in PFM mode with a minimum quiescent current to maintain high efficiency. The converter will position the output voltage typically +1% above the nominal output voltage. This voltage positioning feature minimizes voltage drops caused by a sudden load step.

The transition from PWM mode to PFM mode occurs once the inductor current in the low side MOSFET switch becomes zero, which indicates discontinuous conduction mode.

During the power save mode the output voltage is monitored with a PFM comparator. As the output voltage falls below the PFM comparator threshold of V_{OUT} nominal +1%, the device starts a PFM current pulse. The high side MOSFET switch will turn on and the inductor current ramps up. After the on-time expires, the switch is turned off and the low side MOSFET switch is turned on until the inductor current becomes zero.

The converter effectively delivers a current to the output capacitor and the load. If the load is below the delivered current, the output voltage will rise. If the output voltage is equal or higher than the PFM comparator threshold, the device stops switching and enters a sleep mode with typical 15 μ A current consumption.

If the output voltage is still below the PFM comparator threshold, a sequence of further PFM current pulses are generated until the PFM comparator threshold is reached. The converter starts switching again once the output voltage drops below the PFM comparator threshold.

With a fast single threshold comparator, the output voltage ripple during PFM mode operation can be kept small. The PFM pulse is time controlled, which allows to modify the charge transferred to the output capacitor by the value of the inductor. The resulting PFM output voltage ripple and PFM frequency depend in first order on the size of the output capacitor and the inductor value. Increasing output capacitor values and inductor values will minimize the output ripple. The PFM frequency decreases with smaller inductor values and increases with larger values.

The PFM mode is left and PWM mode entered in case the output current can not longer be supported in PFM mode. The power save mode can be disabled through the MODE pin set to high. The converter will then operate in fixed frequency PWM mode.

8.4.3 100% Duty Cycle Low Dropout Operation

The device starts to enter 100% duty cycle mode once the input voltage comes close to the nominal output voltage. In order to maintain the output voltage, the high side MOSFET switch is turned on 100% for one or more cycles.

With further decreasing V_{IN} the high side MOSFET switch is turned on completely. In this case, the converter offers a low input-to-output voltage difference. This is particularly useful in battery-powered applications to achieve longest operation time by taking full advantage of the whole battery voltage range.

The minimum input voltage to maintain regulation depends on the load current and output voltage, and can be calculated as:

$$V_{INmin} = V_{OUTmax} + (I_{OUTmax} \times (R_{DS(on)max} + R_L))$$

where

- I_{OUTmax} = Maximum output current plus inductor ripple current
- $R_{DS(on)max}$ = Maximum P-channel switch $R_{DS(on)}$
- R_L = DC resistance of the inductor
- V_{OUTmax} = Nominal output voltage plus maximum output voltage tolerance

(1)

Device Functional Modes (continued)

8.4.4 Short-Circuit Protection

The high side and low side MOSFET switches are short-circuit protected with maximum switch current equal to I_{LIMF} . The current in the switches is monitored by current limit comparators. Once the current in the high side MOSFET switch exceeds the threshold of its current limit comparator, it turns off and the low side MOSFET switch is activated to ramp down the current in the inductor and high side MOSFET switch. The high side MOSFET switch can only turn on again, once the current in the low side MOSFET switch has decreased below the threshold of its current limit comparator.

9 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

9.1 Application Information

The TPS6229x devices are high-efficiency synchronous step-down DC/DC converters featuring power save mode or 2.25-MHz fixed frequency operation.

9.2 Typical Application

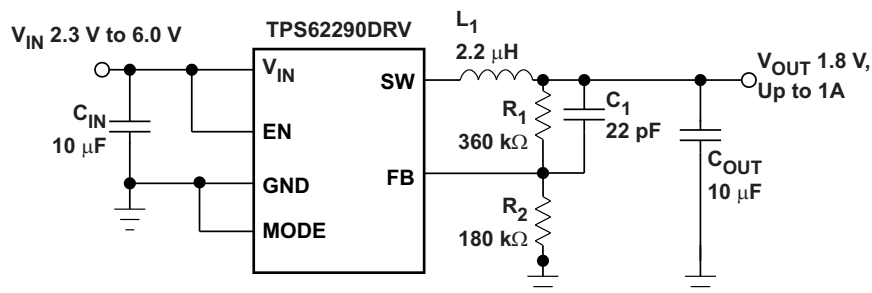


Figure 6. TPS62290DRV Adjustable 1.8 V

9.2.1 Design Requirements

The design guideline provides a component selection to operate the device within the recommended operating condition.

Table 1 shows the list of components for the Application Characteristic Curves.

Table 1. List of Components

COMPONENT REFERENCE	PART NUMBER	MANUFACTURER ⁽¹⁾	VALUE
C _{IN}	GRM188R60J106M	Murata	10 µF, 6.3 V. X5R Ceramic
C _{OUT}	GRM188R60J106M	Murata	10 µF, 6.3 V. X5R Ceramic
C ₁		Murata	22 pF, COG Ceramic
L ₁	LPS3015	Coilcraft	2.2 µH, 110 mΩ
R ₁ , R ₂	Values depending on the programmed output voltage		

(1) See [Third-party Products disclaimer](#)

9.2.2 Detailed Design Procedure

9.2.2.1 Output Voltage Setting

The output voltage can be calculated to:

$$V_{OUT} = V_{REF} \times \left(1 + \frac{R_1}{R_2}\right) \text{ with an internal reference voltage } V_{REF} \text{ typical } 0.6 \text{ V.}$$

To minimize the current through the feedback divider network, R₂ should be 180 kΩ or 360 kΩ. The sum of R₁ and R₂ should not exceed ~1MΩ, to keep the network robust against noise.

An external feed forward capacitor C₁ is required for optimum load transient response. The value of C₁ should be in the range between 22 pF and 33 pF.

Route the FB line away from noise sources, such as the inductor or the SW line.

9.2.2.2 Output Filter Design (Inductor and Output Capacitor)

The TPS6229x is designed to operate with inductors in the range of 1.5 μH to 4.7 μH and with output capacitors in the range of 4.7 μF to 22 μF . The part is optimized for operation with a 2.2- μH inductor and 10- μF output capacitor.

Larger or smaller inductor values can be used to optimize the performance of the device for specific operation conditions. For stable operation, the L and C values of the output filter may not fall below 1- μH effective inductance and 3.5- μF effective capacitance.

9.2.2.2.1 Inductor Selection

The inductor value has a direct effect on the ripple current. The selected inductor has to be rated for its DC resistance and saturation current. The inductor ripple current (ΔI_L) decreases with higher inductance and increases with higher V_{IN} or V_{OUT} .

The inductor selection has also impact on the output voltage ripple in PFM mode. Higher inductor values will lead to lower output voltage ripple and higher PFM frequency, lower inductor values will lead to a higher output voltage ripple but lower PFM frequency.

[Equation 2](#) calculates the maximum inductor current under static load conditions. The saturation current of the inductor should be rated higher than the maximum inductor current as calculated with [Equation 3](#). This is recommended because during heavy load transient the inductor current will rise above the calculated value.

$$\Delta I_L = V_{\text{OUT}} \times \frac{1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}}}{L \times f} \quad (2)$$

$$I_{L_{\text{max}}} = I_{\text{OUT}_{\text{max}}} + \frac{\Delta I_L}{2}$$

where

- f = Switching frequency (2.25 MHz typical)
 - L = Inductor value
 - ΔI_L = Peak-to-peak inductor ripple current
 - $I_{L_{\text{max}}}$ = Maximum inductor current
- (3)

A more conservative approach is to select the inductor current rating just for the maximum switch current of the corresponding converter.

Accepting larger values of ripple current allows the use of low inductance values, but results in higher output voltage ripple, greater core losses, and lower output current capability.

The total losses of the coil have a strong impact on the efficiency of the DC/DC conversion and consist of both the losses in the DC resistance $R_{\text{(DC)}}$ and the following frequency-dependent components:

- The losses in the core material (magnetic hysteresis loss, especially at high switching frequencies)
- Additional losses in the conductor from the skin effect (current displacement at high frequencies)
- Magnetic field losses of the neighboring windings (proximity effect)
- Radiation losses

Table 2. List of Inductors

DIMENSIONS [mm ³]	INDUCTOR TYPE	SUPPLIER ⁽¹⁾
3 × 3 × 1.5	LPS3015	Coilcraft
3 × 3 × 1.5	LQH3NPN2R2NM0	MURATA
3.2 × 2.6 × 1.2	MIPSA3226D2R2	FDK

(1) See [Third-party Products disclaimer](#)

9.2.2.2.2 Output Capacitor Selection

The advanced fast-response voltage mode control scheme of the TPS6229x allows the use of tiny ceramic capacitors. Ceramic capacitors with low ESR values have the lowest output voltage ripple and are recommended. The output capacitor requires either an X7R or X5R dielectric. Y5V and Z5U dielectric capacitors, aside from their wide variation in capacitance over temperature, become resistive at high frequencies.

At nominal load current, the device operates in PWM mode and the RMS ripple current is calculated as:

$$I_{\text{RMS}_{\text{OUT}}} = V_{\text{OUT}} \times \frac{1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}}}{L \times f} \times \left(\frac{1}{2 \times \sqrt{3}} \right) \quad (4)$$

At nominal load current, the device operates in PWM mode and the overall output voltage ripple is the sum of the voltage spike caused by the output capacitor ESR plus the voltage ripple caused by charging and discharging the output capacitor:

$$\Delta V_{\text{OUT}} = V_{\text{OUT}} \times \frac{1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}}}{L \times f} \times \left(\frac{1}{8 \times C_{\text{OUT}} \times f} + \text{ESR} \right) \quad (5)$$

At light load currents the converter operates in power save mode and the output voltage ripple is dependent on the output capacitor and inductor value. Larger output capacitor and inductor values minimize the voltage ripple in PFM mode and tighten DC output accuracy in PFM mode.

9.2.2.2.3 Input Capacitor Selection

The buck converter has a natural pulsating input current; therefore, a low ESR input capacitor is required for best input voltage filtering and minimizing the interference with other circuits caused by high input voltage spikes. For most applications, a 10-μF ceramic capacitor is recommended. The input capacitor can be increased without any limit for better input voltage filtering.

Take care when using only small ceramic input capacitors. When a ceramic capacitor is used at the input and the power is being supplied through long wires, such as from a wall adapter, a load step at the output or V_{IN} step on the input can induce ringing at the V_{IN} pin. The ringing can couple to the output and be mistaken as loop instability or could even damage the part by exceeding the maximum ratings.

Table 3. List of Capacitor

CAPACITANCE	TYPE	SIZE	SUPPLIER ⁽¹⁾
10 μF	GRM188R60J106M69D	0603 1.6 × 0.8 × 0.8 mm ³	Murata

(1) See [Third-party Products disclaimer](#)

9.2.3 Application Curves

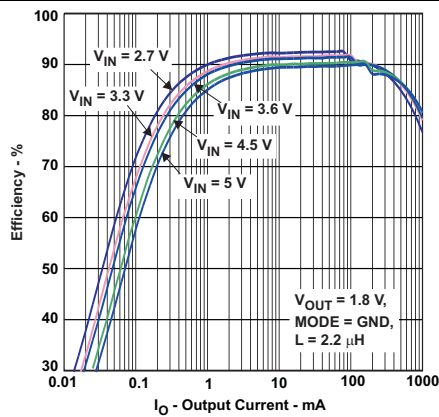


Figure 7. Efficiency (Power Save Mode) vs Output Current, $V_{OUT} = 1.8\text{ V}$

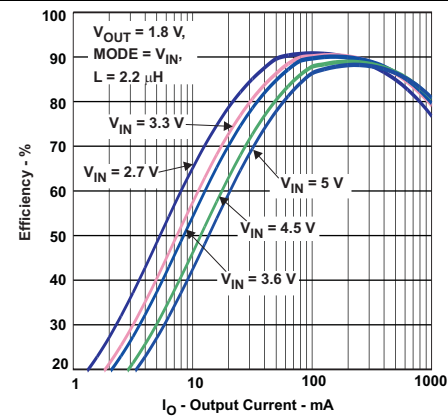


Figure 8. Efficiency (Forced PWM Mode) vs Output Current, $V_{OUT} = 1.8\text{ V}$

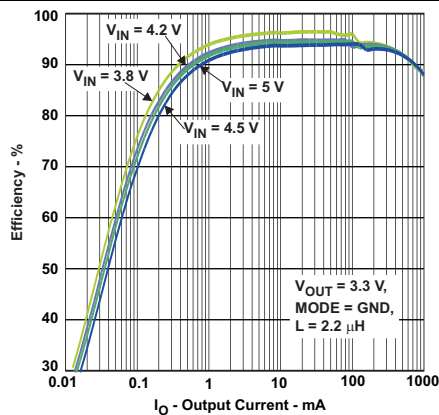


Figure 9. Efficiency (Power Save Mode) vs Output Current, $V_{OUT} = 3.3\text{ V}$

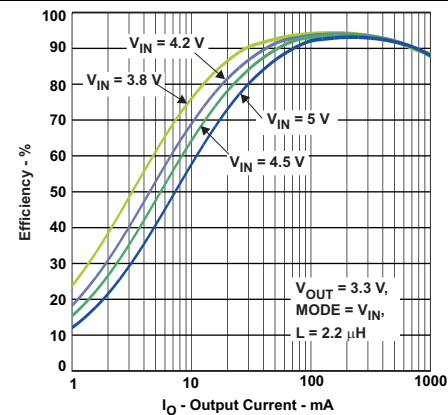


Figure 10. Efficiency (Forced PWM Mode) vs Output Current, $V_{OUT} = 3.3\text{ V}$

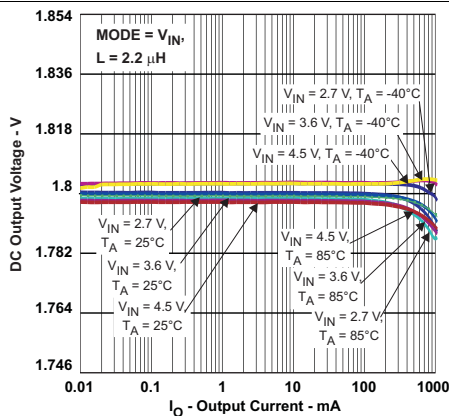


Figure 11. Output Voltage Accuracy (1.8-V Forced PWM Mode) vs Output Current

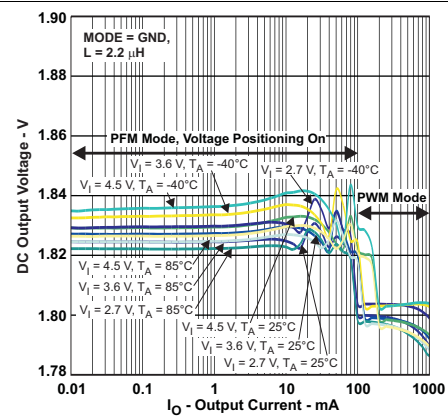


Figure 12. Output Voltage Accuracy (1.8-V Power Save Mode) vs Output Current

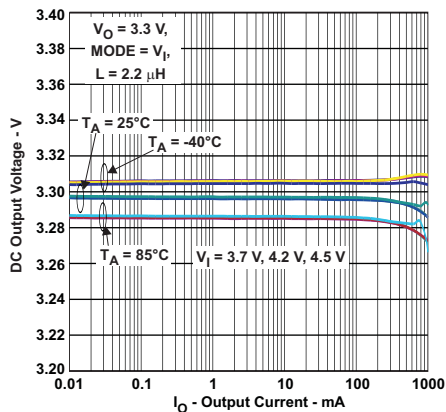


Figure 13. Output Voltage Accuracy 3.3-V Forced PWM Mode vs Output Current

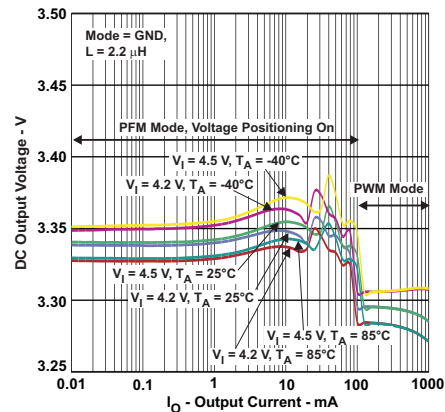


Figure 14. Output Voltage Accuracy 3.3-V Power Save Mode vs Output Current

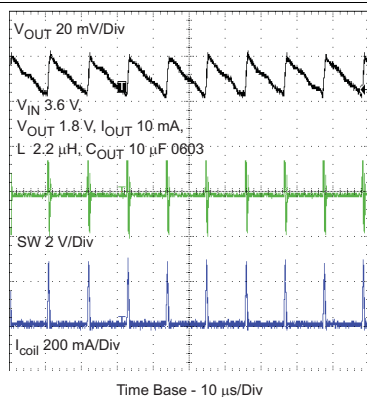


Figure 15. Typical Operation vs PFM Mode

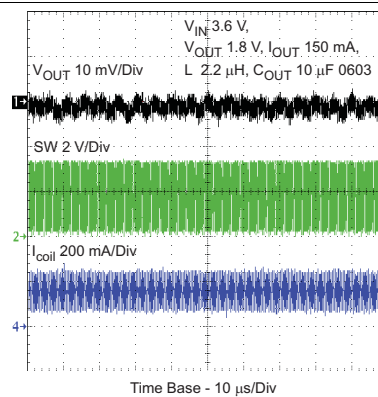


Figure 16. Typical Operation vs PWM Mode

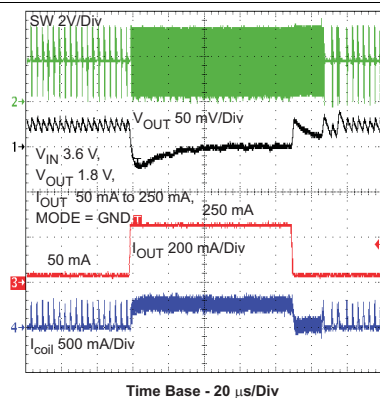


Figure 17. PFM Load Transient

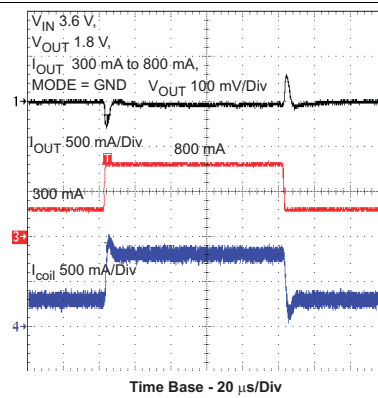


Figure 18. PFM Line Transient

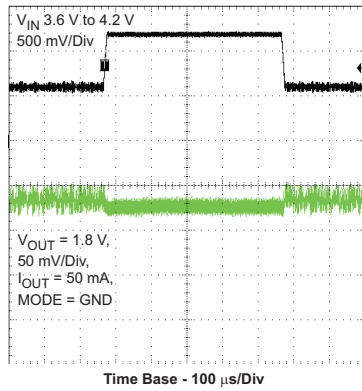


Figure 19. PWM Load Transient

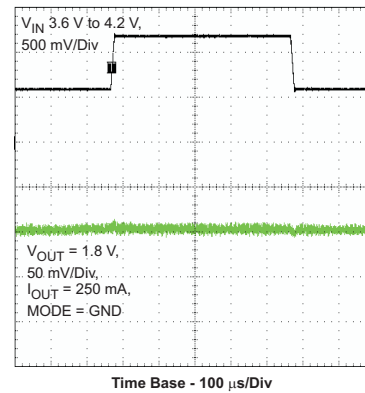


Figure 20. PWM Line Transient

9.3 System Examples

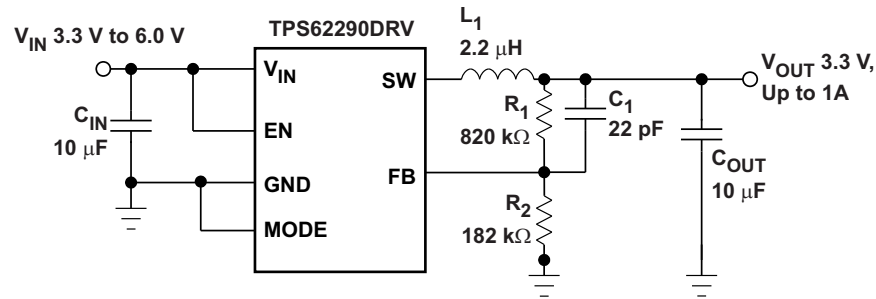


Figure 21. TPS62290DRV Adjustable 3.3 V

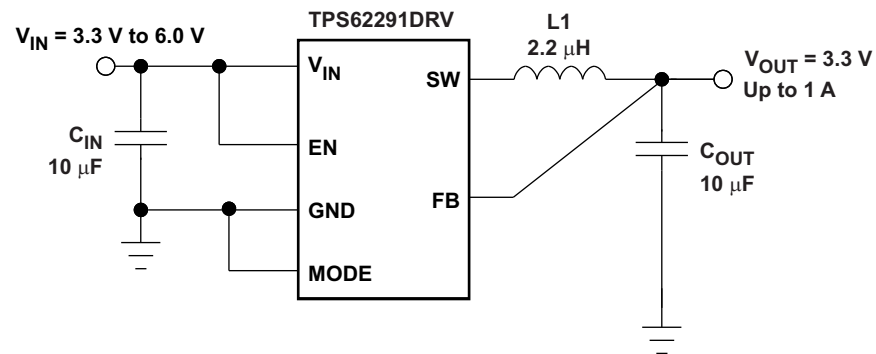


Figure 22. TPS62291DRV Fixed 3.3 V

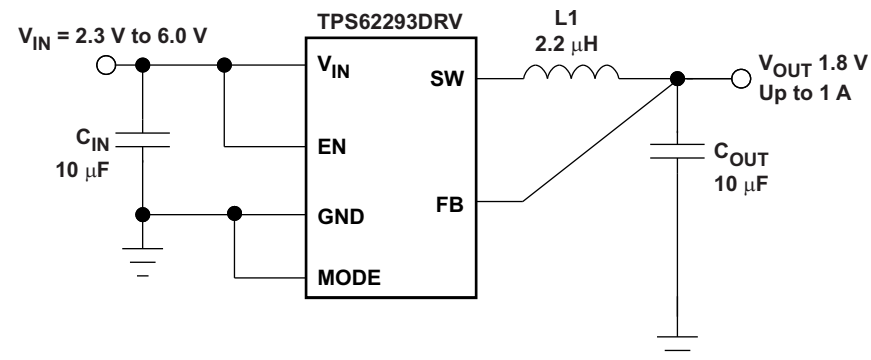


Figure 23. TPS62291DRV Fixed 1.8 V

10 Power Supply Recommendations

The TPS6229x devices have no special requirements for its input power supply. The input power supply's output current needs to be rated according to the supply voltage, output voltage and output current of the TPS6229x.

11 Layout

11.1 Layout Guidelines

As for all switching power supplies, the layout is an important step in the design. Proper function of the device demands careful attention to PCB layout. Care must be taken in board layout to get the specified performance. If the layout is not carefully done, the regulator could show poor line and/or load regulation, stability issues as well as EMI problems. It is critical to provide a low inductance, impedance ground path. Therefore, use wide and short traces for the main current paths. The input capacitor should be placed as close as possible to the IC pins as well as the inductor and output capacitor.

Connect the GND pin of the device to the exposed thermal pad of the PCB and use this pad as a star point. Use a common power GND node and a different node for the signal GND to minimize the effects of ground noise. Connect these ground nodes together to the exposed thermal pad (star point) underneath the IC. Keep the common path to the GND pin, which returns the small signal components and the high current of the output capacitors as short as possible to avoid ground noise. The FB line should be connected right to the output capacitor and routed away from noisy components and traces (for example, SW line).

11.2 Layout Example

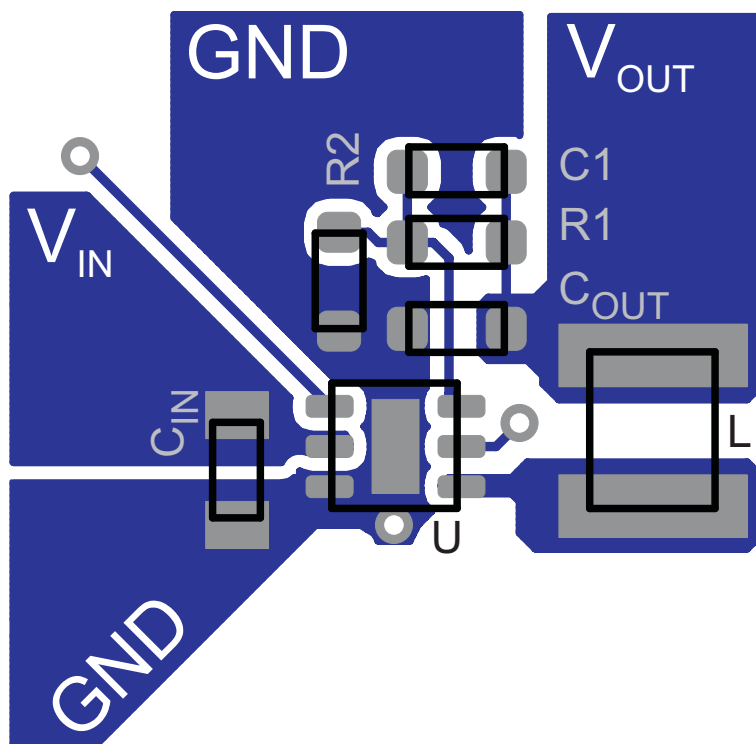


Figure 24. Layout Diagram

12 器件和文档支持

12.1 器件支持

12.1.1 Third-Party Products Disclaimer

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12.2 相关链接

下表列出了快速访问链接。类别包括技术文档、支持和社区资源、工具和软件以及申请样片或购买产品的快速访问链接。

表 4. 相关链接

器件	产品文件夹	样片与购买	技术文档	工具和软件	支持和社区
TPS62290	单击此处	单击此处	单击此处	单击此处	单击此处
TPS62291	单击此处	单击此处	单击此处	单击此处	单击此处
TPS62293	单击此处	单击此处	单击此处	单击此处	单击此处

12.3 社区资源

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设计支持 **TI 参考设计支持** 可帮助您快速查找有帮助的 E2E 论坛、设计支持工具以及技术支持的联系信息。

12.4 商标

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All other trademarks are the property of their respective owners.

12.5 静电放电警告



这些装置包含有限的内置 ESD 保护。存储或装卸时，应将导线一起截短或将装置放置于导电泡棉中，以防止 MOS 门极遭受静电损伤。

12.6 术语表

SLYZ022 — TI 术语表。

这份术语表列出并解释术语、缩写和定义。

13 机械、封装和可订购信息

以下页面包含机械、封装和可订购信息。这些信息是指定器件的最新可用数据。数据如有变更，恕不另行通知，且不会对此文档进行修订。如需获取此数据表的浏览器版本，请参阅左侧的导航栏。

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead finish/ Ball material (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
TPS62290DRVR	ACTIVE	WSON	DRV	6	3000	RoHS & Green	NIPDAUAG	Level-1-260C-UNLIM	-40 to 85	BYN	Samples
TPS62290DRVVT	ACTIVE	WSON	DRV	6	250	RoHS & Green	NIPDAUAG	Level-1-260C-UNLIM	-40 to 85	BYN	Samples
TPS62290DRVVG4	ACTIVE	WSON	DRV	6	250	RoHS & Green	NIPDAUAG	Level-1-260C-UNLIM	-40 to 85	BYN	Samples
TPS62291DRVR	ACTIVE	WSON	DRV	6	3000	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	CFY	Samples
TPS62291DRVVT	ACTIVE	WSON	DRV	6	250	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	CFY	Samples
TPS62293DRVR	ACTIVE	WSON	DRV	6	3000	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	CFD	Samples
TPS62293DRVVG4	ACTIVE	WSON	DRV	6	3000	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	CFD	Samples
TPS62293DRVVT	ACTIVE	WSON	DRV	6	250	RoHS & Green	NIPDAU	Level-1-260C-UNLIM	-40 to 85	CFD	Samples

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBSOLETE: TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

RoHS Exempt: TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.

Green: TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "-" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

⁽⁶⁾ Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

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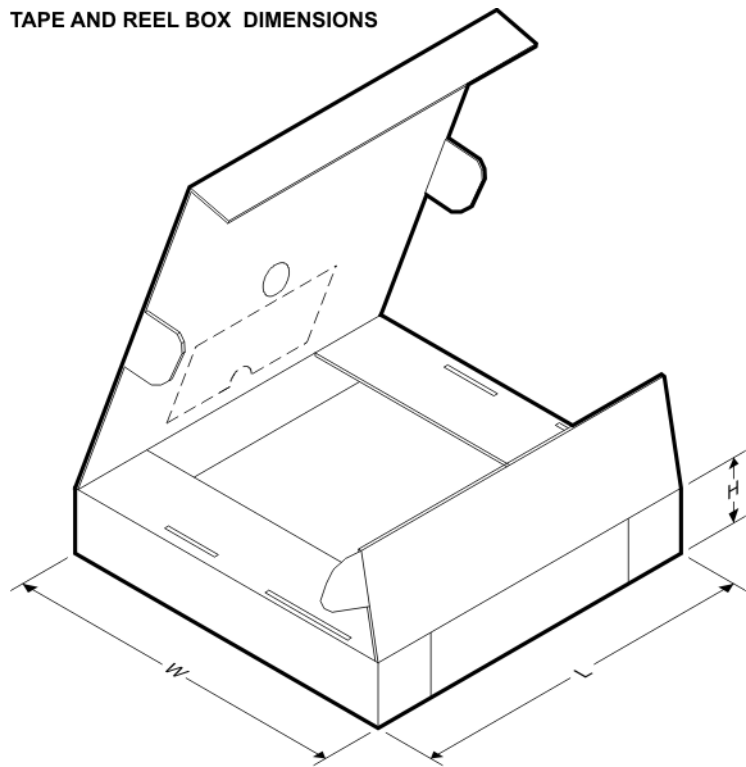
TAPE AND REEL INFORMATION



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS62290DRVR	WSO	DRV	6	3000	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2
TPS62290DRVT	WSO	DRV	6	250	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2
TPS62293DRVT	WSO	DRV	6	250	179.0	8.4	2.2	2.2	1.2	4.0	8.0	Q2

TAPE AND REEL BOX DIMENSIONS

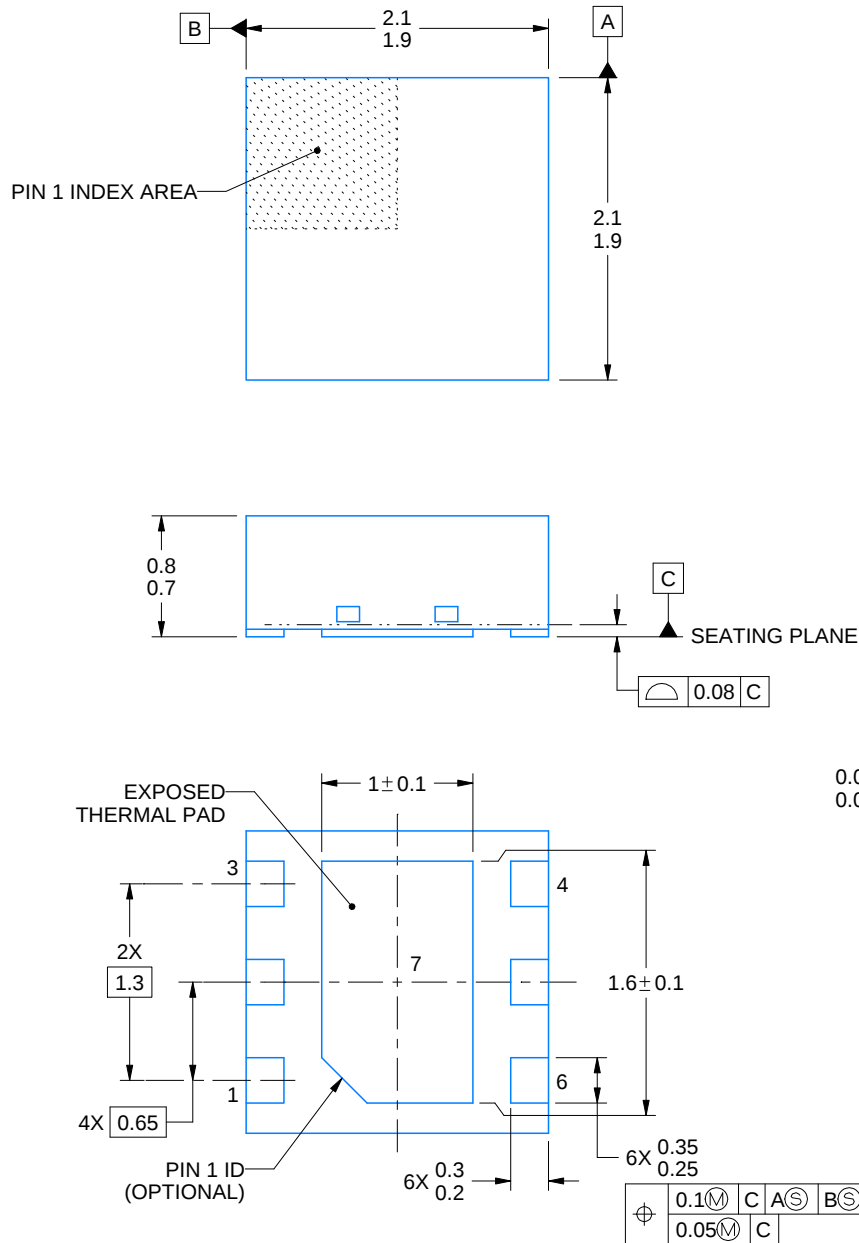
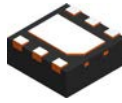


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS62290DRV	WSON	DRV	6	3000	200.0	183.0	25.0
TPS62290DRV	WSON	DRV	6	250	200.0	183.0	25.0
TPS62293DRV	WSON	DRV	6	250	200.0	183.0	25.0



Images above are just a representation of the package family, actual package may vary.
Refer to the product data sheet for package details.



4222173/B 04/2018

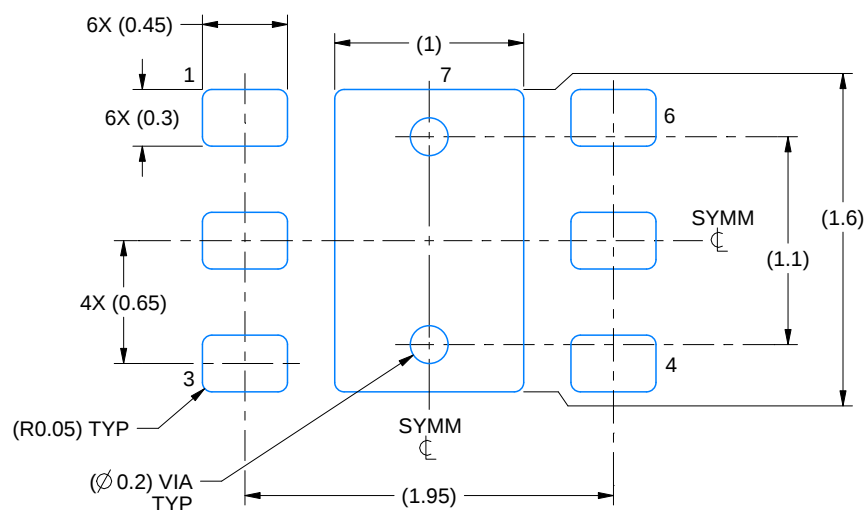
NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.

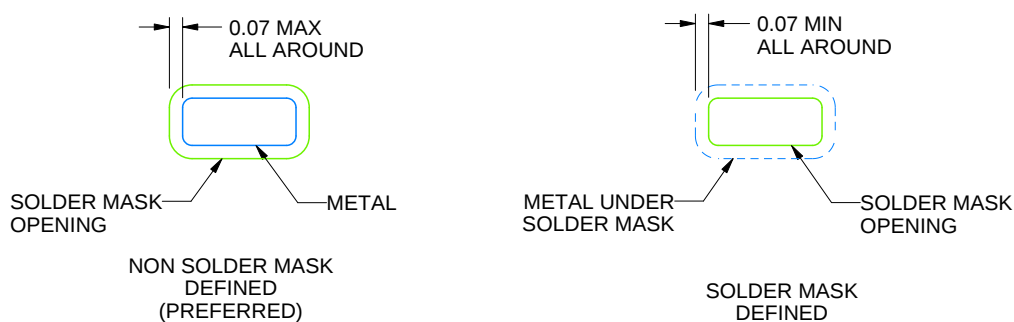
DRV0006A

WSON - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD



LAND PATTERN EXAMPLE
SCALE:25X



SOLDER MASK DETAILS

4222173/B 04/2018

NOTES: (continued)

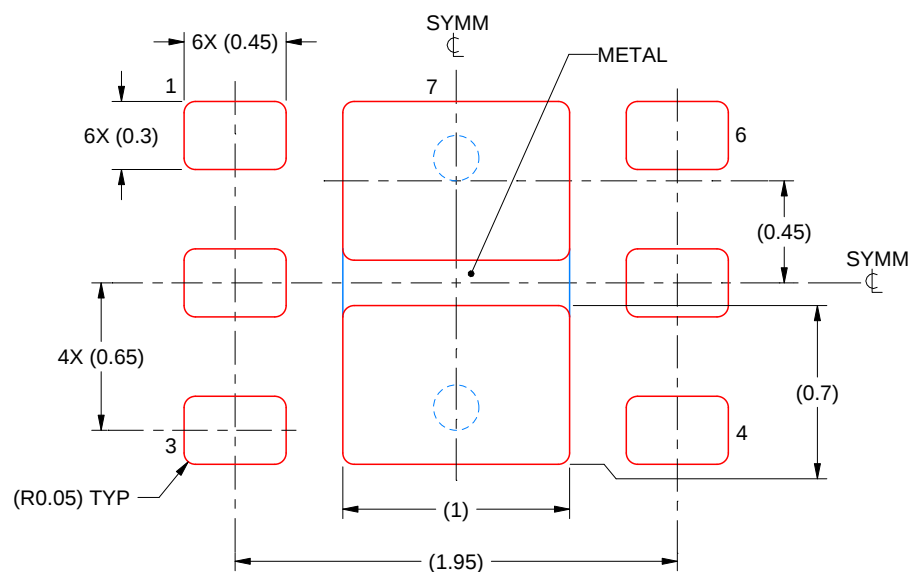
4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 (www.ti.com/lit/slua271).
5. Vias are optional depending on application, refer to device data sheet. If some or all are implemented, recommended via locations are shown.

EXAMPLE STENCIL DESIGN

DRV0006A

WSO - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD



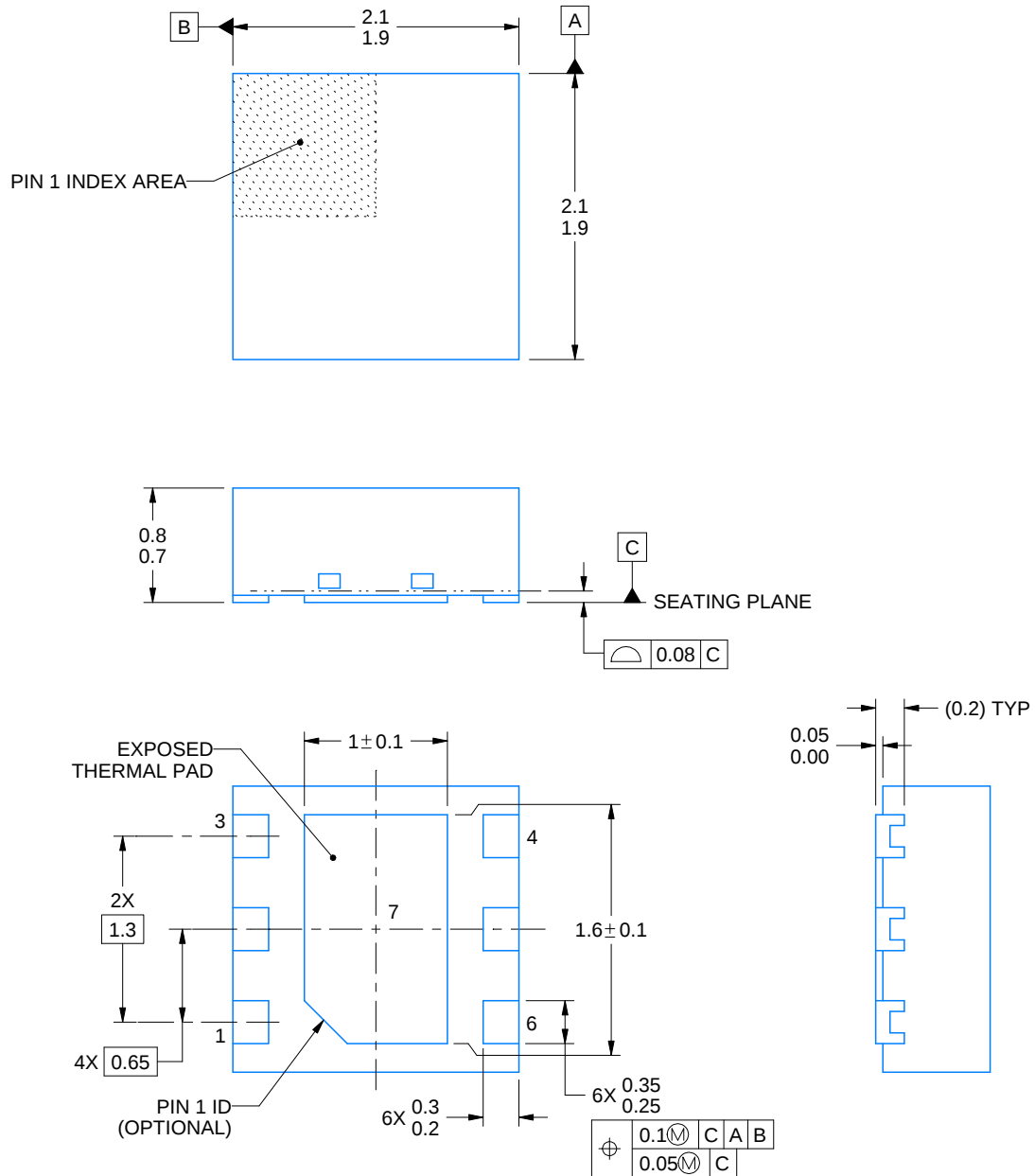
SOLDER PASTE EXAMPLE
BASED ON 0.125 mm THICK STENCIL

EXPOSED PAD #7
88% PRINTED SOLDER COVERAGE BY AREA UNDER PACKAGE
SCALE:30X

4222173/B 04/2018

NOTES: (continued)

6. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.



4225563/A 12/2019

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.

EXAMPLE BOARD LAYOUT

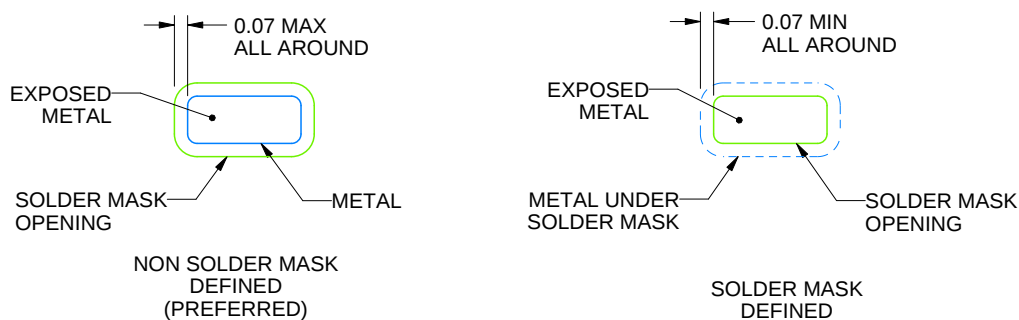
DRV0006D

WSN - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:25X



SOLDER MASK DETAILS

4225563/A 12/2019

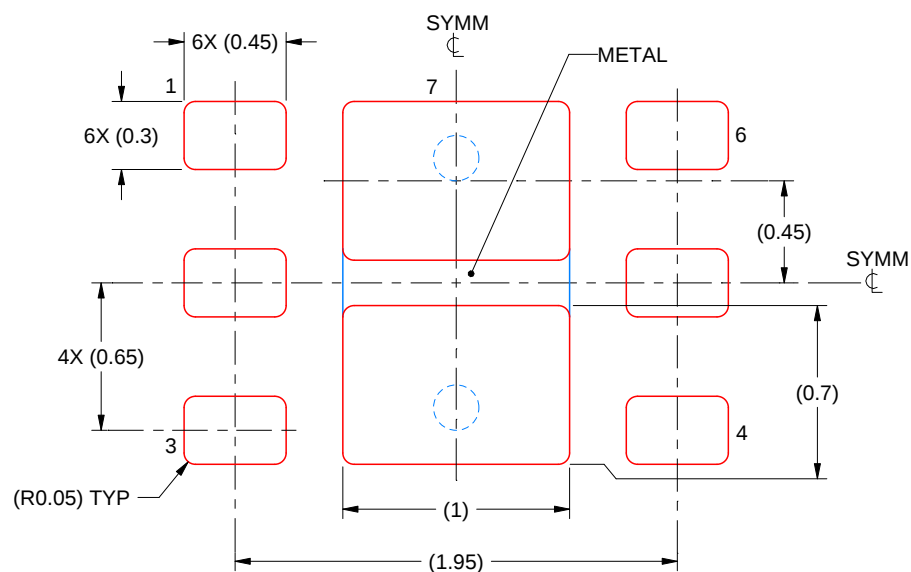
NOTES: (continued)

4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 (www.ti.com/lit/slue271).
5. Vias are optional depending on application, refer to device data sheet. If some or all are implemented, recommended via locations are shown.

DRV0006D

WSN - 0.8 mm max height

PLASTIC SMALL OUTLINE - NO LEAD



SOLDER PASTE EXAMPLE BASED ON 0.125 mm THICK STENCIL

EXPOSED PAD #7
88% PRINTED SOLDER COVERAGE BY AREA UNDER PACKAGE
SCALE:30X

4225563/A 12/2019

NOTES: (continued)

6. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.

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